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A device and method for measuring a property of living
tissue

Cross References to Related Applications

This application claims the priority of international patent application PCT/CH03/00795, filed 2 December 2003, the disclosure of which is incorporated herein by reference in its entirety.

Technical Field

The invention relates to a device for measuring a property of living tissue, in particular the glucose level of the tissue, and a method for doing the same.

Background Art

It has been known that the glucose level in living tissue can be measured non-invasively by applying an electrode arrangement to the skin of a patient and measuring the response of the electrode arrangement to a suitable electric signal. Such a technique is described in WO 02/069791, the disclosure of which is enclosed herein in its entirety.

This type of device is equipped with an electrode arrangement for being applied to the specimen and a voltage-controlled oscillator as a signal source for generating an AC voltage in a given frequency range. The AC voltage is applied to the electrode arrangement. The response of the electrode arrangement, such as a voltage over the electrode arrangement depending on the dielectric properties of the tissue, is fed to a processing circuitry.

Even though this device is well able to monitor glucose, it needs careful calibration and must be operated under well-defined conditions in order to yield results of high accuracy.

The device of WO 02/069791 is one example of a device for measuring a parameter of living tissue. Similar types of devices can be used to measure other properties of the tissue that affect its response to an electric AC field, such as its dielectric constant, or an ion concentration.

Devices of this type should have high accuracy. In addition, in portable devices, low power consumption and low power supply voltages are desired.

Disclosure of the Invention

Hence, in a first aspect of the invention, it is an object to provide a device of this type having low supply voltage.

Now, in order to implement this and still further objects of the invention, which will become more readily apparent as the description proceeds, a device according to claim 1 is used.

In the device according to this aspect of the invention, the voltage-controlled oscillator (VCO) comprises at least one voltage-controlled amplifier the gain of which can be set by a gain control signal. The VCO further comprises at least one tank circuit with a voltage-controlled capacitor determining a frequency of operation of the VCO. The device is adapted to control the gain control signal for increasing the gain when the DC-voltage over the voltage-controlled capacitor(s) is close to zero.

This makes it possible to operate the voltage-controlled capacitor with DC-voltages close to zero where its loss becomes high, thereby allowing to generate

a wide range of frequencies with an only a moderate supply voltage and power consumption.

In a second aspect of the invention, it is an object of the invention to provide a device of the type mentioned above that allows an accurate measurement with simple circuitry.

This second aspect is achieved with the device of claim 7.

In a device according to this aspect, the processing circuitry comprises at least one diode for rectifying an AC input voltage and generating a rectified signal as well as an integrator for smoothing the same. The rectified, smoothed signal (or a signal derived therefrom) is fed to an A/D-converter and converted to a digital value. This digital value will depend on, but not be proportional to, the AC amplitude of the input voltage. Hence, it is converted to a signal value substantially proportional to the AC amplitude of the input voltage, e.g. by means of a calibration function or a lookup table. The wording "substantially proportional" is to designate that the signal value is more proportional to the AC amplitude than the digital value and can be used, at least in approximation, for calculations that require values exactly proportional to the AC amplitude.

In this manner, the analog circuitry is simplified without loss of accuracy. In particular, the analogue circuitry does not need to provide a signal that is exactly proportional to the AC amplitude of the input voltage.

In a second aspect of the invention, it is an object of the invention to provide a device of the type mentioned above, as well as a corresponding method of measurement, that allow an accurate measurement that efficiently exploits the available data.

This second aspect is achieved with the device of claim 14 and the method of claim 29.

In this aspect of the invention, an AC voltage of a series of frequencies f_i is generated and applied to the specimen via the electrode arrangement. A corresponding series of measurement values m_i at each of the frequencies f_i is determined. Each measurement value m_i depends on dielectric properties of the specimen at the corresponding frequency. A function $M(f, b_0, \dots, b_K)$ with parameters b_1 to b_K is fitted to the measurement values m_i at their given frequencies f_i , or through values derived therefrom, thus determining the parameters b_1 to b_K . At least part of the parameters b_1 to b_K can then be used for determining the desired property, e.g. using calibration data from earlier calibration measurements.

Since the involved fitting process exploits information from all used measurement values and inherently compensates for the effects of statistical fluctuations, the results obtained in this way have good accuracy.

In a third aspect of the invention, it is an object to provide a device of the type mentioned above that allows an accurate measurement.

This second aspect is achieved with the device of claim 19.

This aspect is based on the finding that an asymmetric design of the outer electrode provides a stronger, more reliable signal.

In a last aspect of the invention, it is an object to provide a device of the type mentioned above with high physiological compatibility.

This last aspect is achieved by the device of claim 22, where all through-contacts to the electrodes are covered with a biologically inert material. It has been found that through-contacts are a general source of noxious or allergenic substances. Hence, by covering the through-contacts, the biocompatibility of the device can be increased.

It must be noted that the features of the devices according to the various aspects can be used individually or in combination.

Brief Description of the Drawings

The invention will be better understood and objects other than those set forth above will become apparent when consideration is given to the following detailed description thereof. Such description makes reference to the annexed drawings, wherein:

Fig. 1 is a cross section of a device for measuring a glucose level,

Fig. 2 is a block circuit diagram of the device of Fig. 1,

Fig. 3 is a circuit diagram of an advantageous embodiment of a voltage-controlled oscillator,

Fig. 4 is a circuit diagram of an advantageous embodiment of a measuring circuit,

Fig. 5 is the dependence of the digital value at output o1 on the AC amplitude at input u1,

Fig. 6 shows a typical series of measurement values m_1 (dots) and a curve fitted through the values,

Fig. 7 a bottom view of the device of Fig. 1,

Modes for Carrying Out the Invention

Basic setup of the device:

Fig. 1 shows a cross section of a device 100 for measuring a subjects's glucose level. It must be noted, though, that the same type of device can be measure any other parameter of living tissue that affects the response of the tissue to an applied electric AC field as mentioned above. Apart from the glucose level, such a property can e.g. be an electrolyte level of the tissue.

The device of Fig. 1 comprises a housing 1 closed on one side by an electrode plate 2. A display 3 is located opposite electrode plate 2. Electronic circuitry is arranged between electrode plate 2 and display 3.

Electrode plate 2 comprises a flat, electrically insulating substrate 4. A strip electrode 5 covered by an insulating layer 5a and an outer, annular electrode 6, which encloses strip electrode 5 at least partially or fully, are arranged on an outer side 7 of insulating substrate 4. An inner side 8 of insulating substrate 4 is covered by a ground electrode 9. A plurality of through-contacts 10 connect outer electrode 6 to ground electrode 9. A further through-contact 11 connects one end of strip electrode 5 to a contact pad 12 arranged on inner side 8.

A first temperature sensor 15 is mounted to ground electrode 9 in direct thermal contact thereto. The large number of through-contacts 10 ensures that ground electrode 9 closely follows the temperature of outer electrode 6 and therefore the temperature of the specimen, the surface of which is indicated by a dotted line 16.

Leads or springs 18 are provided to connect ground electrode 9, contact pad 12 and first temperature sensor 15 to the electronic circuitry arranged on a printed circuit board 19 forming an assembly of electronic components. Printed circuit board 19 is advantageously arranged on a side of the device that is substantially opposite to the side of electrode plate 2. A battery 21 for powering the circuitry is arranged between printed circuit board 19 and electrode plate 2.

A second temperature sensor 22 is arranged on printed circuit board 19 and in direct thermal contact thereto.

The circuitry of device 100 can be the one described in WO 02/069791. An other possible circuit is, however, shown in the block circuit diagram of Fig. 2. It

comprises a voltage-controlled oscillator (VCO) 31 as a signal source for generating a sine wave signal V_{VCO} or another periodic signal of selectable frequency ω . This signal is fed to an amplifier 32, the output of which is connected via a resistor R1 to a signal point 34 and to a first input u1 of a measuring circuit 37. In addition, the output of amplifier 32 is fed directly to a second input u2 of measuring circuit 37. A resonant circuit 35 comprising an inductance L and a capacitor C in series is connected between signal point 34 and ground.

The operation of measuring circuit 37 will be further described below. Its output, which is e.g. the amplitudes and/or relative phase of the AC-voltages at inputs u1 and u2, is fed to a microprocessor 38, which also controls the operation of VCO 31.

Microprocessor 38 further samples the first and second temperature signals T1, T2 from first and second temperature sensors 15, 22. It also controls display device 3, an input device 40 with user operable controls, and an interface 41 to an external computer. A memory 42 is provided for storing calibration parameters, measurement results, further data as well as firmware for microprocessor 38. At least part of memory 42 is non-volatile.

Inductance L of the device of Fig. 2 can be generated by a coil and/or by the leads and electrodes of capacitor C. Its value is generally known with reasonable accuracy.

Capacitor C of the device of Fig. 2 is formed between strip electrode 5 and outer electrode 6 and is used for probing the specimen. For this purpose, the electrodes are arranged on the skin 16 of the subject as shown in Fig. 1.

For a good and permanent contact with the subject's skin, the device is advantageously worn on an arm or leg and provided with a suitable holder or wrist band 43.

In summary, the device shown in Figs. 1 and 2 comprises:

- a voltage-controlled oscillator for generating an AC voltage in a given frequency range,
- an electrode arrangement comprising the electrodes 5 and 6,
- processing circuitry including the elements 31 - 33, 37, 38 for measuring the response of the electrode arrangement to an electrical signal and deriving the glucose level or some other parameter therefrom.

In addition, it can comprise at least two temperature sensors 15, 22, the signals of which depend in different manner on the skin temperature of the body and on the environmental temperature. One or, advantageously, both these temperatures can be taken into account when determining the glucose level.

Method of operation:

The basic principle of operation of the device is described in WO 02/069791.

To measure the concentration of glucose in the body fluid of the patient, microprocessor 38 can e.g. initiate a measurement cycle consisting of a frequency sweep of VCO 1. The sweep should start at a frequency f_{\max} above the expected resonance frequency f_0 of the resonant circuit 35 and extend to a frequency f_{\min} below resonance frequency f_0 (or vice versa). During this sweep, the electrical properties of the resonant circuit will change. The amplitude determined by measuring circuit A will fall to a minimum A_0 at a characteristic frequency f_0 , as described in WO 02/069791. Similarly, the phase shift ϕ will cross zero.

Microprocessor 38 measures A_0 and/or f_0 , or some other parameter(s) descriptive of the frequency response of the device, as input values describing the physiological state of the subject's blood, body liquids and tissue. In addition to the input values of A_0 and/or

f0, microprocessor 38 measures the temperature values T1 and T2 as further input values. Using suitable calibration data, the glucose level can be derived from these input values.

Such calibration data can be determined from calibration measurements over a range of input values in straightforward manner using methods known to the person skilled in the art.

In general, microprocessor 38 will use a formula of the type

$$g = F(s_1, s_2, \dots, s_N, a_0, a_1, \dots, a_M) \quad (1)$$

for determining the glucose level g (or a parameter indicative thereof) from N measured input values s_1, s_2, \dots, s_N ($N > 0$), where the function F has $M+1$ parameters a_0, a_1, \dots, a_M ($M \geq 0$), at least some of which have to be determined in the calibration measurements.

The measured input values s_i are e.g. values directly or indirectly derived from the amplitude A_0 , the corresponding frequency f_0 , and the temperatures T_1, T_2 . The input values can e.g. be the most recent values measured or they can be a time average or a median over a given number of recent measurements. Possible input values are discussed in the section "Further processing of the raw signals" below.

The function F can be empirical or it can be based at least partially on a model describing the physical nature of the mechanisms involved.

Assuming that the relation between the glucose level g and the measured values s_i is linear at least on approximation, we have

$$g = a_0 + a_1 \cdot s_1 + a_2 \cdot s_2 + \dots + a_N \cdot s_N \quad (2a)$$

with $M = N$.

Equation (2a) has the advantage of being linear in the input values s_i as well as the parameters a_j ,

which simplifies calibration as well as evaluation. More refined models can, however, be used as well.

In order to determine the parameters $a_0, a_1 \dots a_N$, a series of at least $N+1$ calibration measurements has to be carried out, each calibration measurement comprising a determination of the input values s_j and a reference glucose level g measured by conventional means, e.g. an invasive method.

In a most simple approach, the parameters a_i can then be obtained from a conventional least-squares fitting algorithm that varies the parameters a_i in order to find a best match of equations (2) or (2a) to the calibration measurements. Suitable algorithms are known to a person skilled in the art and are e.g. described by Press, Teukolsky, Vetterling and Flannery in "Numerical Recipes in C", Cambridge University Press, 2nd edition, 1992, Chapter 15.

Once the parameters a_i are known, the glucose level g can be determined from equations (2) or (2a) based on the measurement of the input values s_j .

Re-calibration of at least part of the parameters may be advisable at regular intervals or after a displacement of device 100 in respect to the specimen.

In the following, various advantageous aspects of the present device are described in more detail.

Voltage-controlled oscillator:

In principle, various designs of voltage-controlled oscillators are suited for being used in the present device, such as the one shown in Fig. 9 of WO 02/069791. In the following, though, an advantageous embodiment of a voltage-controlled oscillator is described, which operates with low supply voltage, has low power consumption, can oscillate in a large frequency range and generates sine-wave signals with only little distortions.

The voltage-controlled oscillator 31 of Fig. 3 comprises two symmetric tank circuits with inductances L1 and L2 and voltage-controlled capacitors (varactor diodes) D1, D2, respectively. The capacitance of the voltage-controlled capacitors D1, D2 is controlled by a frequency control voltage or frequency control signal V1. In addition, VCO 31 comprises two amplifiers each consisting of a dual-gate FET T1, T2. The gain of transistors T1, T2 is controlled by a gain control voltage or gain control signal V2. The components L1, D1, L2, D2 and T1, T2 are connected to oscillate at the resonant frequency of the tank circuits such that the voltages at the drains of T1, T2 are 180° out of phase. The drains of transistors T1, T2 and therefore the amplifier outputs are interconnected through capacitors C1, C2 and the primary winding of a transformer TR. The secondary winding of transformer TR generates the output voltage V_{VCO} in respect to analog ground AGND (which lies approximately at 2.5 Volts).

The frequency of VCO 31 can be selected via frequency control voltage V1, which can e.g. be generated by microprocessor 38. Typically, frequency control voltage V1 ranges between -10 and +5 Volts. However, when coming close to +5 Volts, the DC-voltage over D1 and D2 decreases and therefore the losses in D1, D2 increase. To compensate for these losses, the gain of the amplifiers is adjusted depending on the value of frequency control voltage V1, by increasing gain control voltage V2 and therefore the amplifier gain when the DC-voltage over voltage-controlled capacitors D1, D2 is close to 0.

Gain control voltage V2 may be generated by microprocessor 38. For example, microprocessor 38 can access calibration data in RAM/ROM 42 that gives, for each value of frequency control voltage V1, a suitable value of gain control voltage V2 or of a derivative thereof.

Advantageously, gain control voltage V2 is generated by a feedback loop that monitors the amplitude

of output voltage V_{VCO} or the signal at second input u_2 of measuring circuit 37 and controls gain control voltage V_2 to keep the amplitude constant. This will again lead to an increase in gain control voltage V_2 when the DC-voltage over voltage-controlled capacitors D_1 , D_2 comes close to 0.

Controlling voltage V_2 in a feedback loop has the advantage that the output voltage is kept substantially constant even if the operating parameters of VCO 31 vary e.g. depending on temperature and/or circuit age. This is particularly important if measuring circuit 37 is designed for optimum performance over a certain voltage range only, and it ensures that nonlinearities of the response of the body to the applied electric field do not affect the measured signals.

The feedback loop for controlling V_2 can be implemented using analog circuitry or with the aid of microprocessor 38. Using microprocessor 38 is advantageous because the circuit design is simplified. However, care must be taken that the implementation of the feedback loop does not unnecessarily increase the power consumption of the device.

Hence, an advantageous implementation of the feedback loop should avoid unnecessarily long operation of the VCO in order to find an appropriate value of V_2 . As mentioned above, microprocessor 38 can initiate a measurement cycle consisting of a frequency sweep of VCO 31. The sweep e.g. starts at a frequency f_{\max} and extends to a frequency f_{\min} and consists of repetitive measurements at a given series of frequencies f_i . In an advantageous embodiment, RAM/ROM 42 holds calibration data that allows to calculate, for each frequency f_i , the derivative $d(f_i) = dV_2/df|_{f=f_i}$. Using this data, the following steps are taken to control the value of voltage V_2 :

- In the first measurement cycle at frequency $f_1 = f_{\max}$, the value of V_2 is varied by microprocessor 38

until voltage u_2 is at a given value u_{2opt} of e.g. 500 mV. The corresponding value of V_2 is $V_2(f_1)$.

- In the second measurement cycle, the value of $V_2(f_2)$ is calculated from $V_2(f_1)$ by linear extrapolation using the derivative $d(f_1)$ (or $d(f_2)$ or a value between $d(f_1)$ and $d(f_2)$), e.g. $V_2(f_2) = V_2(f_1) + (f_1 - f_2) \cdot d(f_1)$.

- In subsequent measurement cycles, $V_2(f_{i+1})$ is calculated again by linear extrapolation from $V_2(f_i)$, but the linearly extrapolated value is corrected by a correction, the value of which depends on if voltage u_2 at frequency f_i was above or below the desired value u_{2opt} . If voltage u_2 at frequency f_i was above u_{2opt} , the correction of $V_2(f_{i+1})$ is aimed to decrease voltage u_2 at frequency f_{i+1} and vice versa. For example, the relation $V_2(f_{i+1}) = V_2(f_i) + k \cdot (f_i - f_{i+1}) \cdot d(f_i)$ can be used for k either being $9/8$ or $7/8$ depending on the comparison of u_2 with u_{2opt} at frequency f_i , or $V_2(f_{i+1}) = k' \cdot (V_2(f_i) + (f_i - f_{i+1}) \cdot d(f_i))$ with k' being slightly above or below 1. This ensures that voltage u_2 remains within a certain range around its optimum value u_{2opt} .

Hence, in general, in at least some of the measurement cycles i , a comparison of the output voltage of VCO 31 (or, equivalently, a voltage derived therefrom, such as voltage u_2) with an optimum value (u_{2opt}) is carried out. The voltage V_2 of a next measurement cycle $i+1$ is then corrected depending on the result of the comparison.

Instead of, or in combination with, a feedback loop for voltage V_2 , RAM/ROM 42 can hold temperature dependent calibration data for calculating a suitable value of voltage V_2 at different frequencies and temperatures, and the temperature measured by temperature sensor 22 can be used to select the appropriate calibration data.

The symmetric design of VCO 31 with two amplifiers T1 and T2 and two tank circuits L1, D1 and L2,

D2 operating at a phase shift of 180° and the fact that the output voltage V_{VCO} is derived from the voltage drop over the outputs of the amplifiers lead to a sine signal with very low distortions. This is of particular importance if the device is to operate over a frequency range of more than 1:2. Depending on the design of measuring circuit 37, higher harmonics would otherwise give rise to additional signals leading to erroneous results.

A typical frequency range of the voltage-controlled oscillator as shown in Fig. 3 is 20 to 60 MHz for a frequency control voltage V_1 of +5 to -10 Volts. The value of gain control voltage V_2 is chosen to be approximately +4 Volts for V_1 close to +5 Volts and +3 Volts for V_1 much smaller than +5 Volts.

As can be seen from Fig. 3, both control voltages are smoothed by capacitors C_3 , C_4 , which act as filters to block any frequencies in the operating range of VCO 31, thereby making the oscillator signal more sinusoidal. For the same purpose, the gates connected to gain control voltage V_2 are connected to the sources of the FETs by means of a filter capacitor C_5 . In addition, and again for the same purpose, the resistor R_1 connected between 0V and the sources of transistors T_1 , T_2 and acting as an approximate current source is arranged parallel to a capacitor C_6 , which again suppresses any oscillations of the resistor voltage at the range of frequencies of VCO 31.

Measuring circuit 37:

In general, measuring circuit 37 can be any circuit that is able to measure the absolute or relative AC amplitudes of the signals at the inputs u_1 and u_2 .

An advantageous embodiment of the measuring circuit is shown in Fig. 4. It comprises two identical channels for processing the signals at the two inputs u_1 ,

u2. In the following, therefore, only the first channel for input u1 is discussed.

The signal at first input u1 is fed to an amplifier A10, the output of which is applied to two diodes D10, D11. Each diode generates a rectified signal at point P10 or P11, respectively. The rectified signal is connected to a capacitor C10 or C11 and a resistor R10 or R11, respectively, which act as an integrator or low pass filter and only pass frequencies much lower than the oscillator frequency f, thereby smoothing the rectified signals. Upper diode D10 is in series to upper filter C10, R10, and upper filter C10, R10 is connected to a first voltage (e.g. +5V). They generate a voltage at point P10 that depends on the minimum value of the AC signal. Lower diode D11 is in series to lower filter C11, R11, and lower filter C11, R11 is connected to a second voltage (e.g. 0V). The second voltage is lower than the first voltage. They generate a voltage at point P11 that depends on the maximum value of the AC signal.

Assuming that the voltage at input u1 is

$$U(t) = U_0 + x \cdot \sin(2\pi ft + \phi), \quad (3)$$

the voltage at point P10 after upper diode D10 is therefore $k \cdot (U_0 - x) + u_d$, wherein k is the gain of amplifier A10 and u_d is the forward voltage of diode D10 at the given frequency and temperature, while the voltage at point P11 after lower diode D11 is $k \cdot (U_0 + x) - u_d$.

The voltages at points P10 and P11 are fed to an instrumental amplifier A11, which yields, at its output a voltage equal to or proportional to the difference of the voltages at its input. An A/D-converter is used to convert this voltage to a digital value o1. The digital value is proportional to $u_d - k \cdot x$ assuming that the response of all devices is linear.

In general, taking into account that the response of some of the elements is not linear and that

some parameters of the circuit, such as the forward voltage u_d , depend on temperature T , frequency ω and/or amplitude x , we have, for the digital value $o1$

$$o1 = H(x, \omega, T), \quad (4)$$

where the response function H is qualitatively depicted in Fig. 5 for two different temperatures T and T' .

In a further processing step, a value proportional to the AC-amplitude x is required. Hence, microprocessor 38 is used for calculating the inverse of function H . For this purpose, the response function H can be determined in calibration measurements and its inverse can be stored as calibration data, e.g. in a table in RAM/ROM 42 for a plurality of temperatures T , frequencies f and AC amplitudes x . For each measurement, microprocessor 38 determines the digital value $o1$ as well as the temperature T (e.g. using second temperature detector T22) and the current frequency ω (which it knows because it controls the operation of VCO 31 by means of frequency control voltage $V1$). Once the values of $o1$, ω and T are known, the value of x can be determined by interpolation from the table stored in RAM/ROM 42.

Instead of using a separate temperature detector T22, the temperature can also be determined from the temperature-dependent forward voltage u_d of one or both of the diodes D10, D11. For this purpose, VCO 31 is switched off, in which case the digital value $o1$ is approximately equal to $2 \cdot u_d$ (where u_d is the forward voltage at frequency 0 and dependent on temperature T).

Instead of using two diodes D10, D11, only a single diode and its corresponding resistor C11 and R11 would suffice, in which case instrumental amplifier A11 or A21 can be dispensed with or be replaced by a simple amplifier. The circuitry of Fig. 1 has, however, the advantage of generating a twice as high signal. In addi-

tion, the symmetric design provides a more accurate result.

Further processing of the raw signals:

For the following steps, we assume that the electrode arrangement 5, 6 is connected to the output of VCO 31 via a first non-zero impedance Z_1 (in the embodiment of Fig. 2, we have $Z_1 = R_1$, but Z_1 may also be an inductive, capacitive or mixed impedance). Hence, the voltage at the electrode arrangement 5, 6 depends on the dielectric properties of the specimen to be measured as well as on the output voltage V_{VCO} from VCO 31. The AC-voltage at input u_1 is derived from or equal to the voltage at the electrode arrangement 5, 6 and therefore also depends on the property of the specimen to be measured as well as, linearly, on the output voltage V_{VCO} from VCO 31.

The input u_2 is connected via a second impedance Z_2 to the output of VCO 31. Z_2 may be zero (as in the embodiment of Fig. 2) or non-zero. The AC-voltage at input u_2 is, at least in good approximation, not dependent on the dielectric properties of the specimen to be measured, but it does depend linearly on the output voltage V_{VCO} from VCO 31.

As described in WO 02/069791, a relative amplitude A between the AC voltages at inputs u_1 and u_2 is preferably used for further processing because such a relative amplitude is not dependent on the absolute amplitude of the output voltage V_{VCO} of VCO 31. This relative amplitude A is

$$A = x_1/x_2, \quad (5)$$

where x_1 is the AC amplitude at input u_1 and x_2 is the AC amplitude at input u_2 . Equivalently, the reciprocal value x_2/x_1 can be used.

As mentioned above, microprocessor 38 can initiate a measurement cycle consisting of a frequency sweep of VCO 1. The sweep should start at a frequency f_{\max} above the expected resonance frequency f_0 of the resonant circuit 35 and extend to a frequency f_{\min} below the resonance frequency f_0 . During this frequency sweep, repetitive measurements of the values x_1 and x_2 are carried out at a given series of frequencies f_i using the circuitry described above. In each measurement i , at least one measurement value m_i is determined. Typically, several hundred measurements are carried out in each measurement cycle.

The measurement values m_i are, in general, a function g of one or both amplitudes x_1 and x_2 :

$$m_i = g(x_{1i}, x_{2i}), \quad (6)$$

where x_{1i} and x_{2i} are the values of x_1 and x_2 measured in measurement i at a frequency f_i . Preferably, for the reasons mentioned above, m_i should be derived from the relative amplitude A only, i.e. from the ratio of the amplitudes x_1 and x_2 , i.e.

$$m_i = G(x_{1i}/x_{2i}) \quad (7)$$

with G being any suitable function, including the identity function. For example, one of the following definitions for the measurement value m_i can be used

$$m_i = x_{1i}/x_{2i} - 1. \quad (8a)$$

or

$$m_i = x_{1i}/x_{2i}. \quad (8b)$$

Since the impedance of the resonant circuit 35 of Fig. 2 goes to a minimum at its resonance frequency f_0 , a typi-

cal series of measurement values m_i looks as shown in Fig. 6.

Part of the input values s_i of equations (1) and (2a) are to be derived from the measurement values m_i . In a simple approach, as it is described in WO 02/069791, a possible input value is the frequency f_0 where x_1/x_2 is smallest and the corresponding minimum value A_0 .

However, in an advantageous embodiment, the following procedure is used.

In a first step, a theoretical or empirical function $M(f, b_0, \dots, b_K)$ with parameters b_1 to b_K is fitted through the points $m_i(f_i)$. Suitable algorithms are known to a person skilled in the art and are e.g. described by the standard textbook of Press et al. mentioned above.

In order to reduce the processing expense and/or to improve the accuracy of the measurement, the measured values m_i can be preprocessed before fitting, e.g. by removing outliers or by numerical smoothing. In that case, the actual fitting process does not use the raw values m_i and f_i but values derived therefrom.

After determining the parameters b_j in the fitting process, at least some of the input values s_i are derived from at least some of the parameters b_j . For example, s_1 can be set to b_0 , s_2 can be set to b_1 etc., or b_0 through b_K can be used to calculate the resonance frequency f_0 and the value of function M at f_0 and the two values obtained in this way can be used as input values s_1 and s_2 , respectively.

In a simple embodiment, a polynomial of third degree is used for function M , i.e.

$$M(f, b_0, \dots, b_K) = b_0 + b_1 \cdot f + b_2 \cdot f^2 + b_3 \cdot f^3 \quad (9)$$

is used. Polynomials of degree R with $R > 3$ or $R = 2$ can be used as well, but it has been found that polynomials

of lower degree do not describe a possible asymmetry of the data sufficiently well, and the available data does not provide sufficient information for determining more than four parameters.

As known to a person skilled in the art and as described in chapter "General Linear Least Squares" in the book of Press et al. mentioned above, fitting a function that is linear in its parameters b_i , such as the one of equation (9), to a data set can be carried out by solving the matrix equation

$$(A^T \cdot A) \cdot b = A^T \cdot m, \quad (10)$$

where, for the function of equation (9), A is the matrix

$$A_{ij} = f_i^j, \quad (11)$$

b is the vector of the parameters $\{b_0 \dots b_K\}$ and m the vector of the values $\{m_1 \dots m_L\}$. In general, when function M takes the form

$$M(f, b_0, \dots, b_K) = \sum_{k=0}^K b_k \cdot \chi_k(f) \quad (12)$$

with χ_k being arbitrary functions of frequency f , matrix A_{ij} is given by

$$A_{ij} = \chi_j(f_i) \quad (13)$$

(Equations (11) and (13) assume that the measurement errors of all measurements are equal. If not, the equations must be corrected as described in the textbook of Press et al., chapter 15.4. In the following, as well as in the claims, the simple form of equations (11) and (13) is used, but the application of error corrected formulae for A_{ij} is deemed to be an equivalent thereof.)

As can be seen, matrix A does not depend on the measured values m_i but only on the frequencies f_i . If the same frequencies f_i are used in each sweep, matrix A as well as $(A^T \cdot A)$ and its inverse can be precalculated and stored in advance, thereby obviating the need for calculating them for each frequency sweep and taking computational load from microprocessor 38, which allows to increase the number of sweeps and/or to decrease power consumption. Preferably, $(A^T \cdot A)^{-1} \cdot A^T$ is precalculated and stored, but it is also possible to store any other suitable data describing the precalculated matrix A .

Electrode design:

The geometry of the electrodes 5, 6 is selected such that the electric AC-field generated by them extends into the tissue to be measured. Advantageously, at least one of the electrodes of the capacitor is electrically insulated such that capacitor C attached to the body, which can be modeled as a resistive and capacitive load, results primarily a capacitive load, the capacitance and loss of which depend on the electrical properties (i.e. the response) of the specimen at the frequency of VCO 1.

The design of the electrodes 5, 6 of the present sensor can correspond to the one described in reference to Figs. 2 and 4 of WO 02/069791, which description is enclosed by reference herein.

In an advantageous embodiment, though, an electrode arrangement as shown in Fig. 7 is used. In this figure, the hatched area corresponds to the area covered by insulating layer 5a, while the dotted areas correspond to the areas covered by electrodes 5 and 6.

As can be seen, outer electrode 6 is of elongate shape having two lateral sections 6a, 6b extending substantially parallel to strip electrode 5, wherein section 6b is wider than section 6a. An inner edge 6c of

outer electrode 6 encloses a central area 50 of substantially rectangular shape. Strip electrode 5 is located substantially in the center of central area 50.

Insulating layer 5a covers substantially all of central area 50 as well as part of the wider lateral section 6b of outer electrode 6.

Any surface of an electrode that can come into contact with the specimen should be of gold or another noble metal for best biological compatibility. In the embodiment of Fig. 7, at least outer electrode 6 is advantageously covered by a gold layer.

For the same reason, at least those through-contacts 10 that are not covered by insulating layer 5a should be covered by glass, ceramics, plastics, a noble metal layer or any other biologically inert material. In the embodiment of Fig. 1, the through-contacts 10 are therefore covered by drops of glass 51.

Notes:

In the above description, the voltage over resonant circuit 35 was measured at input u1. It must be noted, though, that it would also be possible to measure another voltage or current that depends on the impedance of the electrode arrangement. In particular, it would be possible to measure the voltage drop over resistor R1 or inductance L instead of the voltage over resonant circuit 35.

In any case, the processing circuitry 37, 38 should measure a response of the electrode arrangement to the applied electric signal, i.e. the measured value should depend on the dielectric properties of the specimen at the electrode.

Furthermore, resonant circuit 35 might also be implemented as a capacitor parallel to an inductance instead of having the capacitor arranged in series to the inductance.

Finally, it must be noted that the electrode arrangement shown in Figs. 1 and 7 is only one of various possible embodiments. For example, outer electrode 6 might be replaced by a part of the (metallic) housing 1 of device 100 extending to the electrode face of the device. In that case, metallic housing 1 would form part of the electrode arrangement.

While there are shown and described presently preferred embodiments of the invention, it is to be distinctly understood that the invention is not limited thereto but may be otherwise variously embodied and practiced within the scope of the following claims.